

PRACTICAL REALIZATION OF ELECTRONICALLY ADJUSTABLE UNIVERSAL FILTER USING COMMERCIALY AVAILABLE IC-BASED VDBA

Natchanai Roongmuanpha – Tattaya Pukkalanun – Worapong Tangsrirat*

Department of Instrumentation and Control Engineering, Faculty of Engineering, King Mongkut's Institute of Technology Ladkrabang (KMITL), Bangkok 10520, Thailand

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Abstract:

This paper describes the practical realization of electronically adjustable voltage-mode universal filter with three inputs and single output (TISO) using the commercially available integrated circuit (IC)-based voltage differencing buffered amplifiers (VDBAs). The realization is resistor-less and contains only two VDBAs and two capacitors. The described filter structure can realize all the five standard biquadratic filter functions from the same configuration without needing any component matching criterions. It also exhibits low-output impedance, which enables for easy cascading in voltage-mode operation. Owing to practical VDBA realization, the filter circuit can be easily made electronically tunable with orthogonal ω_0 - Q tuning. The effects of the VDBA non-idealities on the filter performance have been analyzed in detail. To prove the theoretical finding, the performance of the studied circuit was also experimentally measured using the operational transconductance amplifier CA3080 and the operational amplifier LF356 ICs.

1 Introduction

In the area of analog signal processing and circuit design, considerable amount of literature has been paid to the implementation of the active filters using a variety of analog active building blocks (ABBs). In 2008, among various types of analog ABBs, the voltage differencing buffered amplifier (VDBA) and its applications for signal generations were introduced [1-6]. The VDBA belongs to a group of modern ABBs so-called voltage differencing units (VDUs), and it is a voltage counterpart of the conventional current differencing buffered amplifier (CDBA) [7]. In the VDBA, the differential input voltage, rather than current as in CDBA, is converted to the current flowing through the terminal z by the transconductance gain. The voltage across the terminal z is then transferred to the voltage at the terminal w. Since the VDBA is composed of a transconductance amplifier followed by the voltage buffered amplifier, this active element is quite suitable for applications in voltage-mode filters with electronically adjustable property. From considerable literature survey, it is found that several specific realizations of active filter using the VDBAs as ABBs have been reported [8-11]. The circuit of [8] uses only two VDBA components and two floating capacitors to implement voltage-mode universal biquad filter configuration with the three inputs and single output (TISO). Other TISO voltage-mode filter in [9] needs a floating resistor for its realization. In [10], n^{th} -order transfer function synthesizers can realize only general n^{th} -order allpole lowpass voltage responses. As also reported in [11], it is focused on the signal-flow-graph synthesis of general n^{th} -order voltage transfer functions using the VDBAs. However, all the above mentioned solutions utilize the VDBA element based on different technologies like CMOS or BiCMOS, which are not commercially available and accessible in general. Therefore the behavior of the previously developed circuits has been only evaluated by computer simulation results. Also, as noted in [12], the employment of commercially available ICs is of practical advantage for such designs.

* Corresponding author

E-mail address: worapong.ta@kmitl.ac.th

This communication deals with the practical TISO voltage-mode universal biquadratic filter realization using recently popularized VDBA elements. The design shows a simple realization for VDBA using commercially available chips. The realized TISO filter requires only two VDBAs and two capacitors and generates all the five standard second-order filter signals namely, lowpass (LP), bandpass (BP), highpass (HP), band stop (BS) and allpass (AP) with no need to impose component choice. The natural angular frequency (ω_0) and the quality factor (Q) of the proposed TISO filter can be tuned electronically and orthogonally. As desired, the output voltage is obtained at the low-impedance-output terminal, which results in cascadability. The practical consideration due to the non-idealities of the VDBAs has been discussed. To examine the experimental measurements, the filter is realized with commercially available active devices operational transconductance amplifier (OTA) CA3080 and JFET input operational amplifier (Op-Amp) LF356.

2 Description of the VDBA and its practical realization

The symbolic notation of the VDBA is illustrated in Figure 1, where p and n are differential voltage input terminals, z is the current output terminal and w behaves as the voltage tracking terminal. Using the standard notation, the ideal terminal characteristics for the VDBA can be expressed by the following matrix expression:

$$\begin{bmatrix} i_p \\ i_n \\ i_z \\ v_w \end{bmatrix} = \begin{bmatrix} 0 & 0 & 0 & 0 \\ 0 & 0 & 0 & 0 \\ g_m & -g_m & 0 & 0 \\ 0 & 0 & 1 & 0 \end{bmatrix} \begin{bmatrix} v_p \\ v_n \\ v_z \\ i_w \end{bmatrix} \tag{1}$$

where g_m is an effective small-signal transconductance gain of the VDBA. In general, the transconductance g_m can be tuned by externally supplied DC current providing the possibility of electronic tuning of the VDBA-based circuit's parameters. In the above expression, the differential input voltage applied across the p and n terminals ($v_p - v_n$) is converted as a small-signal output current i_z to the high-impedance terminal z. Here, a voltage drop at this z-terminal (v_z) is then transferred to the output voltage v_w via a buffered voltage amplifier with unity amplification gain.

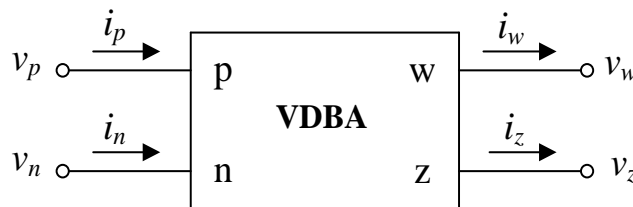


Figure 1. Electrical symbol of the VDBA.

Although the VDBA element is not commercially available as off-the-shelf ICs yet, nevertheless, it can be realized by using other commercially available IC components such as OTA and OA. Figure 2 represents the conception of the VDBA element for practical purposes constructed from commercially available IC devices. In this construction, there is OTA CA3080 by Intersil [13] and Op-Amp LF356 by Texas Instruments [14]. Thanks to the manufactured OTA, an electronic controllability of the transconductance g_m is easily possible, in which its value is in linear dependence on the external DC biasing current I_B . In this case, the value of g_m is determined by:

$$g_m = 20I_B, \tag{2}$$

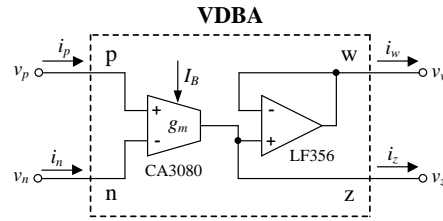


Figure 2. Practical VDBA realization with commercially available CA3080 and LF356 type ICs.

3 Practical TISO electronically adjustable universal filter realization

The realization of an electronically adjustable universal filter with the three input and single output terminals is shown in Figure 3, which consists of the two VDBAs and two floating capacitors C_1 and C_2 . Since the circuit uses only two capacitors as passive components, it is resistorless structure. Through nodal voltage analysis, the output voltage for this TISO filter can be expressed mathematically as:

$$V_{out}(s) = \frac{s^2 C_1 C_2 V_3 + s C_1 g_{m2} V_2 + g_{m1} g_{m2} V_1}{D(s)} \quad (3)$$

where

$$D(s) = s^2 C_1 C_2 + s C_1 g_{m2} + g_{m1} g_{m2} \quad (4)$$

and g_{mi} ($i = 1, 2$) is the transconductance gain associated with the i -th VDBA.

From the above relations, it can be concluded that

- (1) if $V_2 = V_3 = 0$ (grounded) and $V_1 =$ input signal voltage, then the lowpass filter (LP) is realized with V_{out}/V_1 ;
- (2) if $V_1 = V_3 = 0$ and $V_2 =$ input signal voltage, then the bandpass filter (BP) is realized with V_{out}/V_2 ;
- (3) if $V_1 = V_2 = 0$ and $V_3 =$ input signal voltage, then the highpass filter (HP) is realized with V_{out}/V_3 ;
- (4) if $V_2 = 0$ and $V_{in} = V_1 = V_3 =$ input signal voltage, then the bandstop filter (BS) is realized with V_{out}/V_{in} ;
- (5) if $V_{in} = V_1 = -V_2 = V_3$, then the allpass filter (AP) is realized with V_{out}/V_{in} .

Therefore, all the five generic biquadratic filtering functions can be obtained at the V_{out} output terminal of the proposed filter in Figure 3. Owing to the output terminal V_{out} is directly taken from the terminal w of the second VDBA, the proposed filter exhibits the advantageous feature of low output impedance. Note also that there is no any matching component choice for each filter realization.

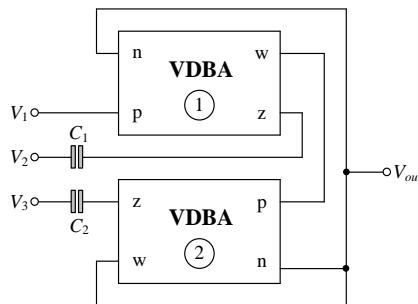


Figure 3. Proposed electronically tunable universal filter.

According to eq. (3) and (4), the natural angular frequency (ω_o), and the quality factor (Q) of the filter are obtained as, respectively:

$$\omega_o = 2\pi f_o = \sqrt{\frac{g_{m1} g_{m2}}{C_1 C_2}} \quad (5)$$

and

$$Q = \sqrt{\frac{g_{m1}C_2}{g_{m2}C_1}} \quad (6)$$

From the above expressions, they reveal that the ω_o -value can be adjusted without disturbing the Q -value by setting the ratio of (g_{m1}/g_{m2}) or (C_2/C_1) invariant. Similarly, the parameter Q can also be tuned independently from the parameter ω_o by keeping the product of $(g_{m1}g_{m2})$ or (C_1C_2) invariant. Therefore, the mentioned TISO configuration of Figure 3 has orthogonal controllability for the important filter parameters ω_o and Q .

4 Non-ideality effect and circuit sensitivity analysis

For the practical consideration, the effects of the VDBA non idealities are to be considered. In case of the non-ideal VDBA, its terminal characteristics given in eq. (1) can be rewritten as:

$$\begin{bmatrix} i_p \\ i_n \\ i_z \\ v_w \end{bmatrix} = \begin{bmatrix} 0 & 0 & 0 & 0 \\ 0 & 0 & 0 & 0 \\ \alpha g_m & -\alpha g_m & 0 & 0 \\ 0 & 0 & \beta & 0 \end{bmatrix} \begin{bmatrix} v_p \\ v_n \\ v_z \\ i_w \end{bmatrix} \quad (7)$$

where $\alpha = (1 - \varepsilon_{gm})$ and $\beta = (1 - \varepsilon_v)$. Here, $|\varepsilon_{gm}| \ll 1$ denotes the transconductance inaccuracy factor, and $|\varepsilon_v| \ll 1$ represents the voltage tracking error from z to w terminal, respectively. The effects of the mentioned non-ideal transfer gains of the VDBA modify the denominator $D(s)$ of eq. (4) to

$$D(s) = s^2C_1C_2 + sC_1\alpha_2g_{m2} + \alpha_1\alpha_2\beta_1\beta_2g_{m1}g_{m2} \quad (8)$$

where α_i and β_i refer to the non-ideal parameters α and β of the i -th VDBA. In this case, the ω_o and Q of the filter are now altered to

$$\omega_o = \sqrt{\frac{\alpha_1\alpha_2\beta_1\beta_2g_{m1}g_{m2}}{C_1C_2}} \quad (9)$$

and

$$Q = \sqrt{\frac{\alpha_1\beta_1\beta_2g_{m1}C_2}{\alpha_2g_{m2}C_1}} \quad (10)$$

The influence of variations in active and passive component values on the filter parameters ω_o and Q can be determined by considering relative sensitivity coefficients, which are obtained to be as follows:

$$S_{\alpha_1}^{\omega_o} = S_{\alpha_2}^{\omega_o} = S_{\beta_1}^{\omega_o} = S_{\beta_2}^{\omega_o} = S_{g_{m1}}^{\omega_o} = S_{g_{m2}}^{\omega_o} = 0.5 \quad (11)$$

$$S_{C_1}^{\omega_o} = S_{C_2}^{\omega_o} = -0.5 \quad (12)$$

$$S_{\alpha_1}^Q = -S_{\alpha_2}^Q = S_{\beta_1}^Q = S_{\beta_2}^Q = S_{g_{m1}}^Q = -S_{g_{m2}}^Q = 0.5 \quad (13)$$

and

$$S_{C_1}^Q = -S_{C_2}^Q = -0.5 \quad (14)$$

It can be easily verified from eq. (11)-(14) that all the above relative ω_o and Q sensitivities are independent of the various circuit elements and equal to 0.5 in magnitude. Also note that, for the absolutely stable circuit, the sensitivity values of all ω_o and Q will be no more than unity.

5 Experimental verification of the filter realization and discussions

In this section, the behavior of the filter realization given in Figure 3 has been tested by experimental measurements using Agilent U8031A triple output DC power supply, and KEYSIGHT EDUX1002G digital oscilloscope. For practical implementation of the VDBA shown in Figure 2, the readily available OTA CA3080 and Op-Amp LF356 chips with $\pm 5V$ DC supply voltages have been employed. In all measurements, the capacitor values were taken as: $C_1 = C_1 = 1$ nF.

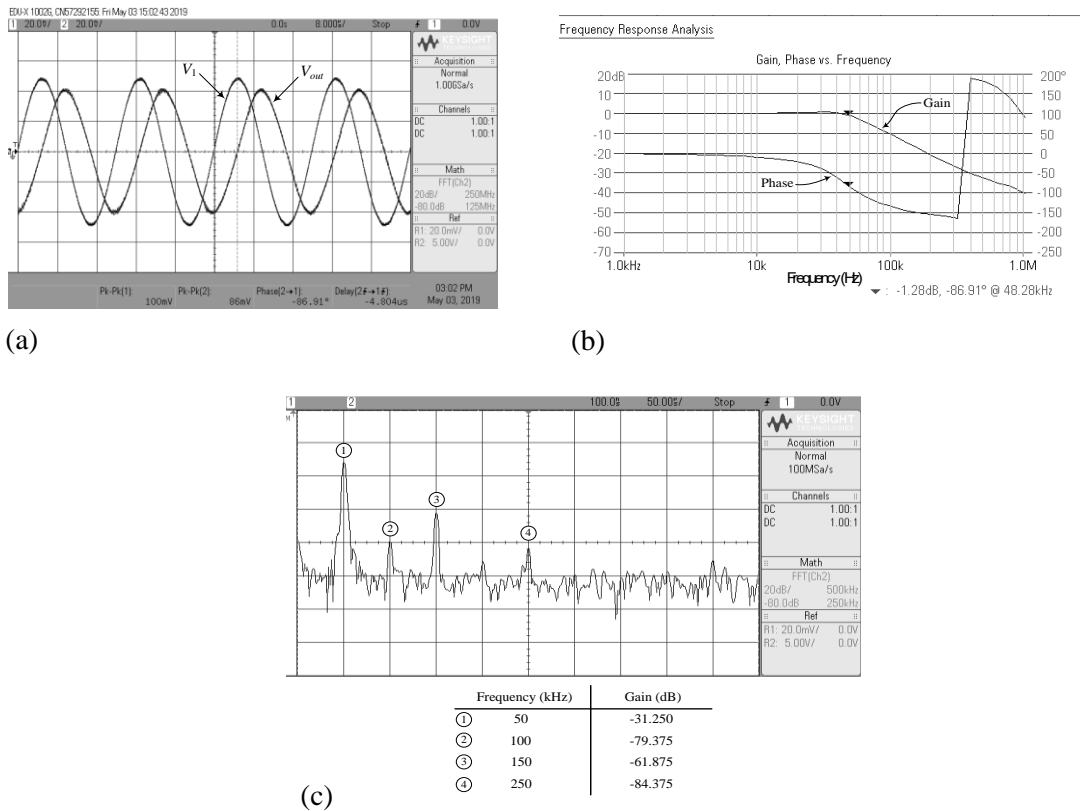
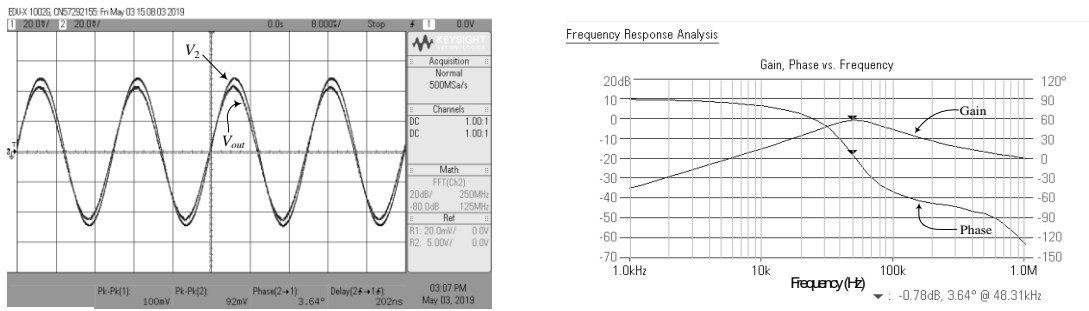


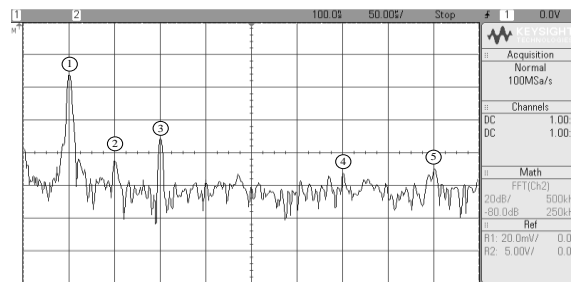
Figure 4. Experimental verification results of the LP filter in Figure 3. (a) time-domain responses (b) measured gain and phase frequency responses (c) frequency spectrum.

As an example to design the filter with the following important characteristics: $f_o = 50$ kHz and $Q = 1$, the experimental component values were set to be: $g_{m1} = g_{m2} \cong 0.31$ mA/V ($I_{B1} = I_{B2} = 15.5$ μA). In time-domain measurements, a 50-mV peak sinusoidal input voltage at the operating frequency of 50 kHz was applied to the filter. The results of the experimental verification for LP, BP, HP, BS and AP filters are respectively depicted in Figure 4-8. From these results, the errors in f_o were measured to be less than 4.82%, and the measured total harmonic distortion (THD) of each filter response is summarized in Table 1. It is, therefore, appeared that the experimental results are found to be agreed with the theoretical values, and they verify the functionality of the realized VDBA-based multifunction filter configuration.



(a)

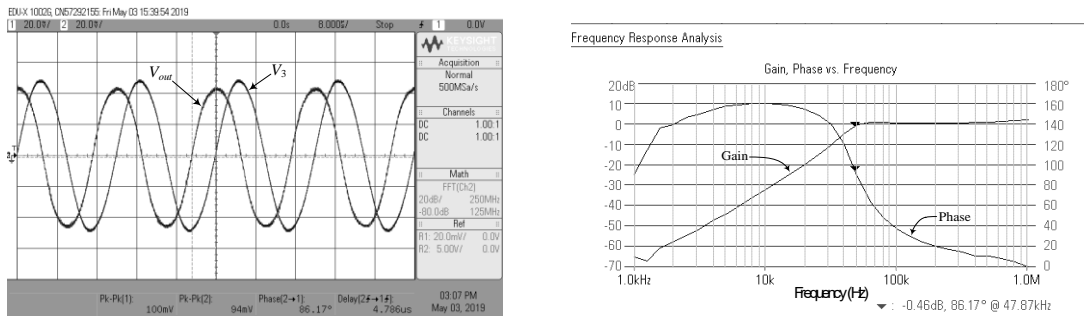
(b)



Frequency (kHz)	Gain (dB)
① 50	-31.875
② 100	-89.375
③ 150	-71.250
④ 350	-92.500
⑤ 450	-91.250

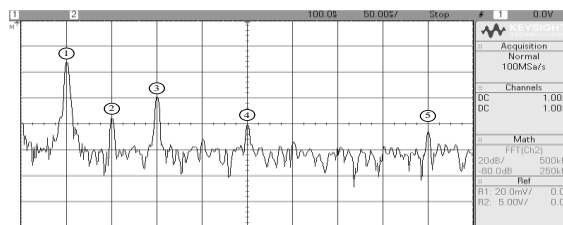
(c)

Figure 5. Experimental verification results of the BP filter in Figure 3. (a) time-domain responses (b) measured gain and phase frequency responses (c) frequency spectrum.



(a)

(b)



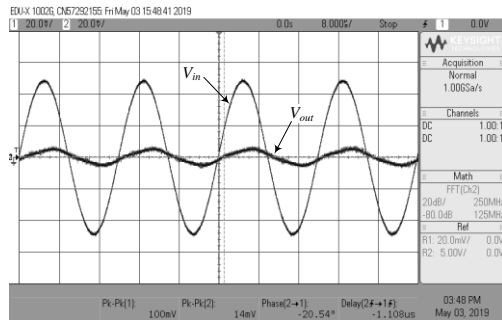
Frequency (kHz)	Gain (dB)
① 50	-31.875
② 100	-75.000
③ 150	-58.750
④ 250	-80.000
⑤ 450	-85.000

(c)

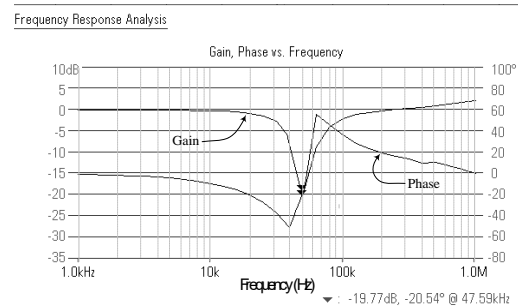
Figure 6. Experimental verification results of the HP filter in Figure 3. (a) time-domain responses (b) measured gain and phase frequency responses (c) frequency spectrum.

Table 1. THD of filter response.

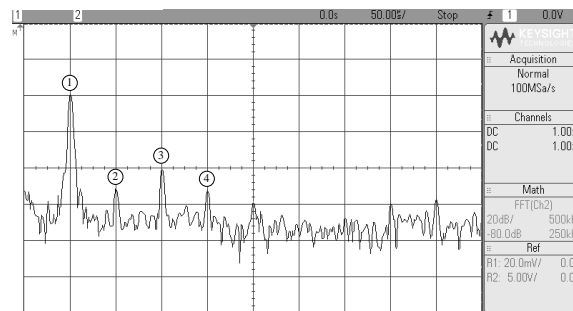
Filter type	THD (%)
LP in Figure 4	2.98
BP in Figure 5	1.09
HP in Figure 6	4.61
BS in Figure 7	0.94
AP in Figure 8	0.98



(a)



(b)

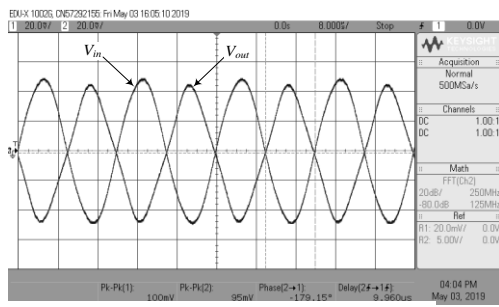


Frequency (kHz)	Gain (dB)
① 50	-39.375
② 100	-91.250
③ 150	-80.625
④ 200	-91.250

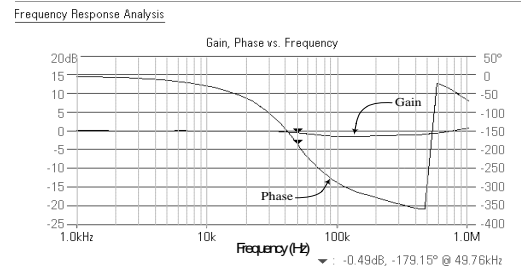
(c)

Figure 7. Experimental verification results of the BS filter in Figure 3. (a) time-domain responses (b) measured gain and phase frequency responses (c) frequency spectrum.

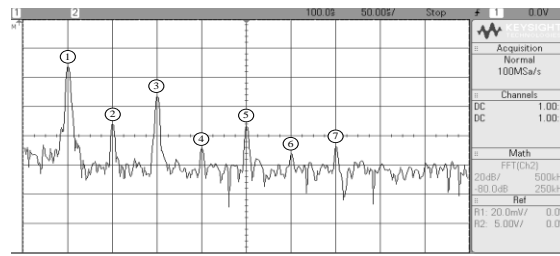
To demonstrate an adjustment of the f_o -value without changing the Q -value, the tuning BP characteristics were observed by changing the supplied currents as depicted in Figure 9. For this purpose, the DC bias currents of the VDBAs were adjusted for three different values, i.e., $I_B = I_{B1} = I_{B2} = 12.5 \mu\text{A}$ ($g_m \cong 0.25 \text{ mA/V}$), $25 \mu\text{A}$ ($g_m \cong 0.50 \text{ mA/V}$), and $31.5 \mu\text{A}$ ($g_m \cong 0.63 \text{ mA/V}$), yielding $f_o = 40 \text{ kHz}$, 80 kHz , and 100 kHz at $Q = 1$. As can be recorded from Figure 9, the corresponding f_o are obtained as: 38.74 kHz , 78.39 kHz and 98.25 kHz , respectively. Figure 10 also shows variation of f_o of the proposed filter on the external control current I_B . Imperfections above these frequencies are attributed to the non-ideal gain effects and parasitic impedances of the active devices and tolerance in nominal value of the capacitor in laboratory test results. However, the proposed filter is proved to be realizable according to the experimental results despite subtle differences observed in theory.



(a)



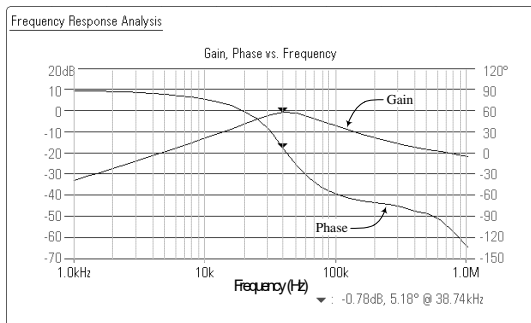
(b)



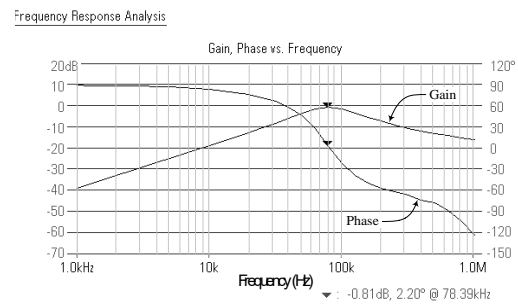
Frequency (kHz)	Gain (dB)
① 50	-31.875
② 100	-71.875
③ 150	-52.500
④ 200	-88.125
⑤ 250	-72.500

(c)

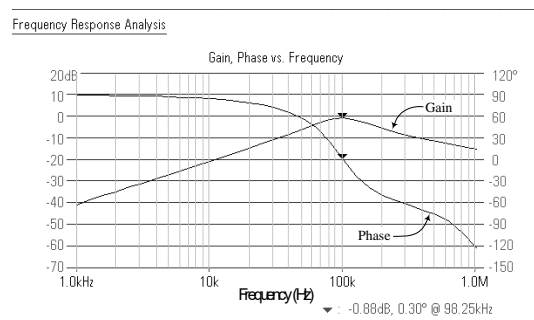
Figure 8. Experimental verification results of the AP filter in Figure 3. (a) time-domain responses (b) measured gain and phase frequency responses (c) frequency spectrum.



(a)



(b)



(c)

Figure 9. Measured BP frequency responses with tuning f_o (a) $f_o = 40$ kHz (b) $f_o = 80$ kHz (c) $f_o = 100$ kHz.

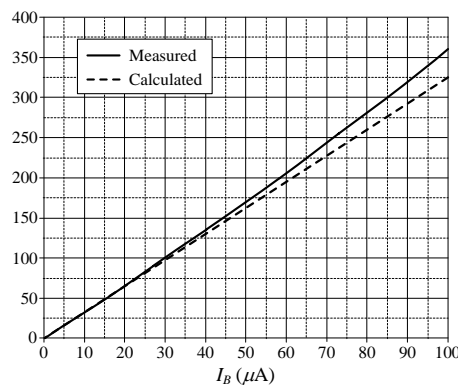


Figure 10. Dependence of f_o on bias current I_B .

6 Comparison with the previously published works

A comparison of the proposed universal filter with the previously similar works published in the literature [15]-[17] is summarized in Table 2. It is observed from Table 2 that both circuits of [15-16] employ external resistors, which are not desired for fully integrated circuit (IC) technology. The circuit of [16] also suffers from the lack of electronic adjustability. Moreover, a DDCC (differential difference current conveyors) in [16] is not available commercially. The work from [17] uses a non-canonical number of active elements, i.e. 6 OTAs (operational transconductance amplifiers) and 2 MOS transistors. Accordingly, it suffers from high-power dissipation and large chip area occupation in ICs. It should be mentioned here that the proposed circuit is only the work that realizes an electronically tunable TISO universal filter using only the VDBA ABBs and capacitors, no passive resistors and does not need any component matching conditions.

Table 2. Comparison of performance of the proposed circuit with other previously published works.

Parameter	[15]	[16]	[17]	This work
Technology	LT1228	0.5- μ m MIETEC	LM13600	LT1228
Supply voltages	$\pm 5V$	$\pm 2.5V$, $-1.7V$	$\pm 5V$	$\pm 5V$
No. of input	3	3	4	3
No. of output	1	1	1	1
Input impedance	high	high	high	high
Output impedance	low	low	low	low
No. active elements	LT1228 = 1	DDCC = 3	OTA = 6 MOS = 2	VDBA = 2
No. passive elements	R = 1 C = 2	R = 2 C = 2	C = 2	C = 2
Matching requirement	no	no	no	no
Electronic adjustability	yes	no	yes	yes
Experimental results	yes	no	no	yes

7 Conclusion

This paper presents the practical possibility of realizing a voltage-mode biquadratic filter with three inputs and one output employing the recently introduced active element named the VDBA. The practical VDBA is realized with standard commercially available chips OTA CA3080 and OP-Amp LF 356. The presented circuit, consisting of only two practical VDBAs together with two capacitors, can realize the five standard biquadratic filter functions all at a single low-impedance-output terminal, without requiring any element-matching condition. It also exhibits the possibility of independent electronics changing of the natural angular frequency

and the quality factor through the VDBA transconductances and has low sensitivity coefficients. The results of breadboard implementation of the proposed filter are also accomplished to validate the theoretical analysis and its practical significance.

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